Performance of Decision Feedback Equalizer over Frequency Selective Fading Channel in W-CDMA Systems

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Abstract—The CDMA systems provide the greater capacity in wireless communication environment. But a major obstacle for this is multipath fading which causes inter symbol interference (ISI). The conventional sub optimum receiver consisting of a bank of matched filters is often inefficient because interference is treated as noise. The device used to combat with ISI is named as equalizer. Among linear and non linear equalizers, non linear equalizer outperforms over linear equalizers. Here decision feedback equalizer is non linear equalizer. This paper considers a non linear equalizer such as decision feedback equalizer (DFE) to mitigate inter symbol interference (ISI) in code division multiple access (CDMA) systems.

Index Terms—Feed-forward and feedback filters, linear adaptive transversal equalizer (LTE), zero-forcing equalizer, direct sequence code division multiple access (DS-CDMA), and correlation.

I. INTRODUCTION

The high flexibility and low cost of wireless communication systems increases demand for them. This led to development of multiple access schemes like wideband DS-CDMA systems [1] to achieve higher capacities. In digital wireless communication systems the major obstacle for reliable communication is inter-symbol interference (ISI), encountered in multipath transmission channels. To compensate the ISI channel equalization is used. The fading effects of multipath channel proportional to the complexity of the equalizer design [2]. The maximum likelihood sequence detection (MLSD) is used to combat with ISI. MLSD uses trellis based Viterbi algorithm [3]. The complexity Viterbi algorithm exponentially increases with number of states in trellis. The number of schemes, generally known as reduced-state sequence estimation (RSSE), were proposed in [4, 5]. The recent research devoted to the receiver design using zero forcing, minimum MSE (MMSE) linear equalization methods combat with multipath fading channels [6, 7]. The decision feedback equalizer minimizes the MSE between the input and decision device. The DFE generally outperforms the traditional linear equalizer, particularly if the channel has deep spectral null in its response.

A decision feedback equalizer based on MMSE criterion provides better performance than linear MMSE equalizers over highly dispersive channel. These findings are motivated to design a chip level DFE for CDMA downlink channel.

To develop this type of system offers numerous challenges. First one is to develop the method for the chip level feedback from symbol decision. The second one is to suppress pre-cursor ISI, post cursor ISI from all users and current symbol interference from other users. The third one is to develop a method to detect signals buried in inter chip interference (ICI). Here ICI is interference between chips caused by frequency selective fading channels.

In this paper section II describes the system model for CDMA systems at transmitter end and also describes the channel model for CDMA systems. Section III describes the equalizers. In this section also derived the MMSE optimum feed-forward filter (FFF) tap weights and feedback filter tap weights. Section IV describes the DFE filter receiver for CDMA systems.

II. SYSTEM MODEL

A. Transmission end for CDMA systems

Consider a base station with J mobile stations in a WCDMA system. The fth user is assigned to fj,m(k) (k=0,1,....,P-1) of length P to spread bit wij(n) at time i. After multiplexing, each mobile station through a common multipath channel. Assume the channel is FIR and has order q (q<P) with q+1 chip rate coefficients. Also assume, we oversample the channel output to generate M sub-channels. If we use hj(n) to represent the nth composite sub-channel impulse response, including the transmitter, the physical channel and the receiver, then the output of the nth sub-channel due to user j is

\[ u_{j,m}(n) = \sum_{l=0}^{q} h_m(l)s_j(n-l) \]  (1)

where

\[ s_j(n) = \sum_{k=-\infty}^{\infty} w_j(k)f_{j,m}(n-kP) \]

The following assumptions are made in respect of codes and symbols mentioned above;

1. The spreading code is an independent identically distributed (i.i.d) white sequence with unit variance.
2. These spread codes are orthogonal to each other.

The BPSK modulated spread signal propagates through a dispersive multipath channel with the impulse response h(t).

The impulse response of a multipath channel can be expressed as

\[ h(t) = \sum_{l=0}^{N-1} h_m(\delta(t-mT_c)) \]  (2)

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The transmission signal and the impulse response of jth user are expressed in (1) & (2). From (4), the received multipath CDMA signals are depicted in figure.1.

The optimum tap weights adaptive linear equalizer is obtained by forcing the main lobe of received signal and all side lobes (ISI terms) to zero, named as zero forcing linear equalizer. The tap weights adaptive linear equalizer is obtained by Minimum Mean Square Error (MMSE) at the output of the linear adaptive equalizer. Linear equalizers do not perform well on channels which have deep spectral nulls in passband. In an attempt to compensate for the linear equalizer places too much gain in the vicinity of the spectral null, thereby enhancing the noise present in those frequencies. The basic idea behind the decision feedback equalization is that once an information symbol has been detected and decided upon, the ISI that it induces on future symbol can be estimated and subtracted out before detection of subsequent symbols. The baseband DFE filter depicted in figure.3.

**III. EQUALIZERS**

Equalization compensates for Inter Symbol Interference (ISI) created by within time dispersive channels. Coherence bandwidth is statistical measure of the range of frequencies over the channel can be considered “flat” (i.e., a channel which passes all spectral components with approximately equal gain and linear phase). If the transmitted signal bandwidth exceeds the coherence band width of radio channel ISI occurs and transmitted signal pulses are spread in time into adjacent symbols. ISI is major obstacle to high speed data transmission over wireless channels. An equalizer within a receiver compensates for the average range of expected channel amplitude and delay characteristics. Equalizers must be adaptive since the channel is generally unknown time varying. The classification of equalizers is depicted in figure.2.
The received signal is equalized using a DFE which consists of a feed-forward filter (FFF) and a feedback filter (FFB). The feed-forward filter has \( L_f \) taps and its impulse response is denoted by the vector \( f = [f(0) \ f(1) \ \ldots \ f(L_f - 1)]^T \) and the feedback filter has \( L_b \) taps and its impulse response is denoted by the vector \( b = [b(0) \ b(1) \ \ldots \ b(L_b - 1)]^T \). Then the input to the de-spreading box can be derived as

\[
y(n+1) = u(n+1) + b(1)[u(n) - d(n)] + z(n)
\]

(6)

Where \( d(n) \) decision box output and \( z(n) \) comprises of modeled post-cursor ISI residual precursor ISI, residual post-cursor ISI, filtered noise. \( Z(n) \) can be expressed as

\[
z(n) = \sum_{i=2}^{L_f} b(i)(u(n-i) - d(n-i)) + \sum_{i=2}^{L_b} c(i)u(n + \Delta - i) + \sum_{i=0}^{L_b-1} f(i)z(n-i).
\]

(7)

Where \( c = h*f \), symbol * denotes convolution operation, is combined impulse response of both channel and feed-forward filter. And \( \Delta \) denotes overall delay caused by system. Assume all previous decisions are correct i.e., \( d(n-1) = u(n-1) \). The output of decision device can be expressed as

\[
d_n = \sum_{l=0}^{L_f} f(l)r(n-l) - \sum_{l=1}^{L_b} b(l)u(n-l - \delta)
\]

(8)

The error and error variance of the signal can be expressed as

\[
e(n) = d(n) - u(n - \delta)
\]

(9)

\[
J = E[e(n)^2]
\]

(10)

Here, invoke the orthogonality principle then the error variance is

\[
J = \int (\phi_{hh} + \sigma_n^2 I) \bar{f}^H + \bar{b}^H \bar{b} + 1 - \bar{f}^H H \bar{b}
\]

- \( \bar{f}^H H \bar{f} \quad \bar{f} - \bar{f}^H h - h^H \bar{f} \)

(11)

To obtain optimum filter weights differentiate \( J \) with respect to \( f^* \) and \( b^* \), respectively, we obtain as \( f_{opt} \) and \( b_{opt} \) as

\[
\bar{f}_{opt} = ((\phi_{hh} - HH^H) + \sigma_n^2 I)^{-1} h
\]

(12)

\[
\bar{b}_{opt} = H^H \bar{b}
\]

(13)

The MMSE of DFE is given by

\[
J = 1 - \bar{f}_{opt}^H h
\]

(14)

The FFF and FBF are cancel the perfectly cancels the residual ISI components

IV. DFE FILTER FOR CDMA SYSTEMS

To mitigate the chip level ISI in CDMA systems, the DFE filter is depicted in figure 4. Here assume that previous detected symbols are correct, \( z(n+1) \) is conditionally uncorrelated to \( [e(n) | y(n)] \). The filtered noise is uncorrelated with the decision error \( e(n) \). The residual ISI components have some correlation with the decision error \( e(n) \), but assume that the correlation is small enough to be ignored.
The bit error rate (BER) response of linear equalizer in CDMA is shown in figure(5). Here the BER response of zero-forcing DFE filter, MMSE DFE filter over AWGN channel compared with the BPSK signal BER performance over AWGN channel.

VI. CONCLUSION

In this paper, decision feedback equalizer using zero-forcing and MMSE criterion developed for CDMA systems, based on correlation technique for channel estimation. It has been shown that the performance MMSE-DFE system is better than zero-forcing DFE and linear equalizer. We would like to investigate this to turbo DFE environment. This issue can taken up as future scope the work.

REFERENCES